

Appendix

Fundamentals of Backstepping Control

This Appendix provides the fundamentals of the recursive backstepping control method. The presented material is a summary of more detailed descriptions that may be found in [43, 49]. Lyapunov-based controller design may be systematically tackled by a recursive design procedure called *backstepping*. Backstepping is suitable for strict-feedback systems that are also known as “lower triangular”. An example of a strict-feedback systems is:

$$\begin{aligned}\dot{\xi}_1 &= f_1(\xi_1) + g_1(\xi_1)\xi_2 \\ \dot{\xi}_2 &= f_2(\xi_1, \xi_2) + g_2(\xi_1, \xi_2)\xi_3 \\ &\vdots \\ \dot{\xi}_{r-1} &= f_{r-1}(\xi_1, \xi_2, \dots, \xi_{r-1}) + g_{r-1}(\xi_1, \xi_2, \dots, \xi_{r-1})\xi_r \\ \dot{\xi}_r &= f_r(\xi_1, \xi_2, \dots, \xi_r) + g_r(\xi_1, \xi_2, \dots, \xi_r)u\end{aligned}\tag{A.1}$$

where $\xi_1, \dots, \xi_r \in \mathbb{R}$, $u \in \mathbb{R}$ is the control input and f_i, g_i for $i = 1, \dots, r$ are known functions. A typical feedback linearization approach in most cases leads to cancellation of useful nonlinearities. The backstepping design exhibits more flexibility compared to feedback linearization since it does not require that the resulting input–output dynamics be linear. Cancellation of potentially useful nonlinearities can be avoided resulting in less complex controllers. The main idea is to use some of the state variables of (A.1) as “virtual controls” or “pseudo controls”, and depending on the dynamics of each state, design intermediate control laws. The backstepping design is a recursive procedure where a Lyapunov function is derived for the entire system. The recursive procedure can be easily expanded from the nominal case of a system augmented by an integrator. This is also referred to as *integrator backstepping*. Based on the design principles of the integrator backstepping, the control design can be easily expanded for the case of strict-feedback systems given by (A.1).

A.1 Integrator Backstepping

The baseline design of the recursive procedure is the *integrator backstepping*. Consider the system:

$$\dot{\eta} = f(\eta) + g(\eta)\sigma \quad (\text{A.2})$$

$$\dot{\sigma} = u \quad (\text{A.3})$$

where $[\eta \ \sigma]^T \in \mathbb{R}^{n+1}$ is the state vector and $u \in \mathbb{R}$ is the control input. The objective is to design a state feedback control law such that $\eta, \sigma \rightarrow 0$ as $t \rightarrow \infty$. It is assumed that both f and g are known. This system can be viewed as a cascade connection of two subsystems. The first subsystem is (A.2) with σ as input and the second subsystem is the integrator (A.3). The main design idea is to treat σ as a virtual control input for the stabilization of η . Assume that there exists a smooth state feedback control law $\sigma = \phi(\eta)$, with $\phi(0) = 0$, such that the origin of:

$$\dot{\eta} = f(\eta) + g(\eta)\phi(\eta) \quad (\text{A.4})$$

is asymptotically stable. Consider that for the choice of $\phi(\eta)$ a Lyapunov function $V(\eta)$ is known such that:

$$\frac{\partial V}{\partial \eta} [f(\eta) + g(\eta)\phi(\eta)] \leq -W(\eta), \quad \forall \eta \in \mathbb{R}^n \quad (\text{A.5})$$

where $W(\eta)$ is positive definite. By adding and subtracting $g(\eta)\phi(\eta)$ on the right hand side of (A.2), one has:

$$\dot{\eta} = f(\eta) + g(\eta)\phi(\eta) + g(\eta)[\sigma - \phi(\eta)] \quad (\text{A.6})$$

$$\dot{\sigma} = u \quad (\text{A.7})$$

Denote by e_σ the error between the state σ and the pseudo control $\phi(\eta)$, that is:

$$e_\sigma = \sigma - \phi(\eta) \quad (\text{A.8})$$

Writing the initial system in the (η, e_σ) coordinates, one has:

$$\dot{\eta} = [f(\eta) + g(\eta)\phi(\eta)] + g(\eta)e_\sigma \quad (\text{A.9})$$

$$\dot{e}_\sigma = u - \dot{\phi}(\eta) \quad (\text{A.10})$$

Since f , g and ϕ are known, one of the advantages of the backstepping design is that it does not require a differentiator. In particular, the derivative $\dot{\phi}$ can be computed by using the expression:

$$\dot{\phi} = \frac{\partial \phi}{\partial \eta} [f(\eta) + g(\eta)\sigma] \quad (\text{A.11})$$

Setting $u = v + \dot{\phi}$, where $v \in \mathbb{R}$ is a nominal control input, the transformed system takes the form:

$$\dot{\eta} = [f(\eta) + g(\eta)\phi(\eta)] + g(\eta)e_\sigma \quad (\text{A.12})$$

$$\dot{e}_\sigma = v \quad (\text{A.13})$$

which is similar to the initial system, except that now the first component has an asymptotically stable origin when the input is zero. Using this procedure, the pseudo control $\phi(\eta)$ has been “back stepped” through the integrator from $u = v + \phi(\eta)$. The knowledge of $V(\eta)$ is exploited in the design of v for the stabilization of the overall system. Using:

$$V_c(\eta, \sigma) = V(\eta) + \frac{1}{2}e_\sigma^2 \quad (\text{A.14})$$

as a Lyapunov function candidate, one obtains:

$$\begin{aligned} \dot{V}_c &= \frac{\partial V}{\partial \eta} [f(\eta) + g(\eta)\phi(\eta)] + \frac{\partial V}{\partial \eta} g(\eta)e_\sigma + e_\sigma v \\ &\leq -W(\eta) + \frac{\partial V}{\partial \eta} g(\eta)e_\sigma + e_\sigma v \end{aligned} \quad (\text{A.15})$$

The control input v is chosen as:

$$v = -\frac{\partial V}{\partial \eta} g(\eta) - ke_\sigma, \quad k > 0 \quad (\text{A.16})$$

Substituting the above choice of v to (A.15), one has:

$$\dot{V}_c \leq -W(\eta) - ke_\sigma^2 \quad (\text{A.17})$$

which shows that the origin ($\eta = 0, e_\sigma = 0$) is asymptotically stable. Since $\phi(0) = 0$, and $e_\sigma \rightarrow 0$ as $t \rightarrow \infty$; then, the, origin ($\eta = 0, \sigma = 0$) is asymptotically stable as well. Substituting for v, e_σ , and ϕ , the final form of the control law is:

$$u = \frac{\partial \phi}{\partial \eta} [f(\eta) + g(\eta)\sigma] - \frac{\partial V}{\partial \eta} g(\eta) - k[\sigma - \phi(\eta)] \quad (\text{A.18})$$

A.2 Example of a Recursive Backstepping Design

This Section illustrates the implementation of the backstepping methodology to a strict feedback system of high order. The construction of the controller for high order systems is based on the recursive implementation of the integrator backstepping methodology. An illustration of the backstepping procedure based on the generic formulation of the strict feedback systems given in (A.1), would result in the derivation of tedious recursive formulas which are difficult to follow. In this Section, a simple third order strict feedback system is used instead. This approach provides a better insight to the key features and potentials of the backstepping design. Consider the following system:

$$\begin{aligned} \dot{\xi}_1 &= f_1(\xi_1) + \xi_2 \\ \dot{\xi}_2 &= f_2(\xi_2) + \xi_3 \\ \dot{\xi}_3 &= u \end{aligned} \quad (\text{A.19})$$

where $\xi_i \in \mathbb{R}$ for $i = 1, 2, 3$ are the system states, $u \in \mathbb{R}$ is the control input and $f_i(\xi_i) : \mathbb{R} \rightarrow \mathbb{R}$ are known functions. The objective is to design a state feedback

control law such that $\xi_1, \xi_2, \xi_3 \rightarrow 0$ as $t \rightarrow 0$. Similarly to the integrator backstepping case, the idea is to use the state variable ξ_2 as an input for the stabilization of ξ_1 . Consider the Lyapunov function $V_1 = \frac{1}{2}\xi_1^2$. The derivative of V_1 along the trajectory of ξ_1 is computed as:

$$\dot{V}_1 = \xi_1(f_1(\xi_1) + \xi_2) \quad (\text{A.20})$$

The objective of this step is to find a control law $\phi_2(\xi_1)$ with $\phi_2(0) = 0$, such that when $\xi_2 = \phi_2(\xi_1)$ then $\dot{V}_1(\xi_1) \leq -W_1(\xi_1)$ where W_1 is a positive definite function for every $\xi_1 \in \mathbb{R}$. An obvious choice would be to remove the effect of the function $f_1(\xi_1)$ and inject a stabilizing feedback term. Thus, we pick:

$$\phi_2(\xi_1) = -f_1(\xi_1) - \kappa_1 \xi_1 \quad (\text{A.21})$$

where κ_1 is a positive gain. This choice yields $\dot{V}_1 \leq -\kappa_1 \xi_1^2$. Denote the error $e_2 = \xi_2 - \phi_2(\xi_1)$. Using the new coordinate e_2 the system given in (A.19) can be written as:

$$\begin{aligned} \dot{\xi}_1 &= -\kappa_1 \xi_1 + e_2 \\ \dot{e}_2 &= -\dot{\phi}_2(\xi_1) + f_2(\xi_1, e_2) + \xi_3 \\ \dot{\xi}_3 &= u \end{aligned} \quad (\text{A.22})$$

Similarly to Sect. A.1, the implementation of the derivative $\dot{\phi}_2(\xi_1)$ does not require a differentiator since:

$$\dot{\phi}_2 = \frac{\partial \phi_2}{\partial \xi_1} [f_1(\xi_1) + \xi_2] \quad (\text{A.23})$$

Let $V_2(\xi_1, e_2) = \frac{1}{2}\xi_1 + \frac{1}{2}e_2^2$. The goal of the second design step is to determine a pseudo control $\phi_3(\xi_1, e_2)$ with $\phi_3(0, 0) = 0$ such that when $\xi_3 = \phi_3(\xi_1, e_2)$ then $\dot{V}_2(\xi_1, e_2) \leq -W_2(\xi_1, e_2)$ where W_2 is a positive definite function for every ξ_1, e_2 . Consequently, the derivative of V_2 along the solutions of ξ_1, e_2 is:

$$\dot{V}_2 = -\kappa_1 \xi_1^2 + e_2(\xi_1 - \dot{\phi}_2(\xi_1) + f_2(\xi_1, e_2) + \phi_3(\xi_1, e_2)) \quad (\text{A.24})$$

An obvious choice would be:

$$\phi_3(\xi_1, e_2) = -\xi_1 + \dot{\phi}_2(\xi_1) - f_2(\xi_1, e_2) - \kappa_2 e_2 \quad (\text{A.25})$$

where κ_2 is a positive constant. In this case $\dot{V}_2 = -\kappa_1 \xi_1^2 - \kappa_2 e_2^2$. Using the change of variables $e_3 = \xi_3 - \phi_3(\xi_1, e_2)$ the system dynamics become:

$$\begin{aligned} \dot{\xi}_1 &= -\kappa_1 \xi_1 + e_2 \\ \dot{e}_2 &= -\xi_1 - \kappa_2 e_2 + e_3 \\ \dot{e}_3 &= -\dot{\phi}_3(\xi_1, e_2) + u \end{aligned} \quad (\text{A.26})$$

Similarly to $\dot{\phi}_2$, the computation of $\dot{\phi}_3$ does not require a differentiator. Using $V_3 = V_2 + \frac{1}{2}e_3^2$ as a candidate Lyapunov function one has:

$$\dot{V}_3 = -\kappa_1 \xi_1^2 - \kappa_2 e_2^2 + e_3(e_2 - \dot{\phi}_3(\xi_1, e_2) + u) \quad (\text{A.27})$$

The choice of u is:

$$u = -e_2 + \dot{\phi}_3(\xi_1, e_2) - k_3 e_3 \quad (\text{A.28})$$

where k_3 is a positive constant. This choice yields:

$$\dot{V}_3 = -k_1 e_1^2 - k_2 e_2^2 - k_3 e_3^2 \quad (\text{A.29})$$

therefore the origin of the error system is globally asymptotically stable. Since $\phi_2(0), \phi_3(0, 0) = 0$ then $\xi_1, \xi_2, \xi_3 \rightarrow 0$ as $t \rightarrow \infty$. The final system dynamics have the form:

$$\begin{bmatrix} \dot{\xi}_1 \\ \dot{e}_1 \\ \dot{e}_2 \end{bmatrix} = \begin{bmatrix} -k_1 & 1 & 0 \\ -1 & -k_2 & 1 \\ 0 & -1 & -k_3 \end{bmatrix} \begin{bmatrix} \xi_1 \\ e_2 \\ e_3 \end{bmatrix} \quad (\text{A.30})$$

As indicated by [49], an important structural property of the above system is that the system matrix is composed by the sum of a negative diagonal and a skew-symmetric matrix. This is a typical structural pattern when the backstepping design is based on a sequential construction of Lyapunov functions. The key feature of the backstepping methodology is the fact that it provides significant design freedom. The choice of the pseudo controls ϕ_2, ϕ_3 and the control input u is not unique. For example, we could have picked:

$$\begin{aligned} \phi_2(\xi_1) &= -f_1(\xi_1) - \kappa_1 \xi_1 \\ \phi_3(\xi_1, e_2) &= \dot{\phi}_2(\xi_1) - f_2(\xi_2) - k_2 e_2 \\ u &= \dot{\phi}_3(\xi_1, e_2) - k_3 e_3 \end{aligned}$$

resulting to the system:

$$\begin{bmatrix} \dot{\xi}_1 \\ \dot{e}_1 \\ \dot{e}_2 \end{bmatrix} = \begin{bmatrix} -k_1 & 1 & 0 \\ 0 & -k_2 & 1 \\ 0 & 0 & -k_3 \end{bmatrix} \begin{bmatrix} \xi_1 \\ e_2 \\ e_3 \end{bmatrix} \quad (\text{A.31})$$

which is obviously asymptotically stable. Thus, the stabilization of the same system can be achieved with a much more simpler design. This potential constitutes the backstepping methodology as a powerful design tool for the development of simplistic controllers for nonlinear systems.

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